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A compact wideband printed antenna for free-space radiometric detection of partial discharge

Yong ZHANG[1,*], Pavlos LAZARIDIS[1], Raed ABD-ALHAMEED[2], Ian GLOVER[1]

[1] Department of Engineering & Technology, University of Huddersfield, Huddersfield, UK

[2] School of Electrical Engineering & Computer Science, University of Bradford, Bradford, UK

*Correspondence: y.zhang@hud.ac.uk

Abstract: A microstrip line-fed wideband printed antenna is presented for radio detection of partial discharge (PD). The novel simple structure antenna has compact size of 24 × 20 × 0.16 cm^3 (0.28λ_s × 0.23 λ_s × 0.002 λ_s) and suitable for radiometric PD wireless sensor nodes, where λ_s is the wavelength of the lowest frequency of the band (i.e., 0.35 GHz). The stepped and beveled radiation patch is used in combination with a slotted ground plane to achieve a wide fractional bandwidth of 119% (0.35 to 1.38 GHz) for a return loss better than 10 dB. Good radiation pattern characteristics are obtained across the frequency band of interest. The match between simulated and experimental results suggests that the design is sound and robust.

Key words: Wideband, compact size, printed antenna, partial discharge, radio detection.

1. Introduction

Partial discharge (PD) may occur when a usually-earthed metallic component in an item of high voltage (HV) plant becomes disconnected from ground. PD monitoring can play a valuable role in the on-going maintenance of HV plant. The location of PD sources by free-space radio detection is an attractive approach for condition monitoring of HV equipment in electricity substations. A suggested band for radio PD detection is 0.3–1.5 GHz [1]. A low-cost, radiometric, PD wireless sensor network (WSN) has been

proposed to provide real-time coverage for an entire substation [2]. The PD WSN is a collection of broadband radiometer sensors that measure PD activity interfaced to WirelessHART modules. The WirelessHART modules relay the PD activity data to an access point via wireless links. The access point is interfaced to a network and security manager and may also be interfaced to network gateway. For such PD detection systems, the design of radiometer antennas is one of the major challenges.

Several antennas for PD detection have recently been reported [1, 3–5]. These antennas, however, address multi-narrow-band operation [1, 4] or achieve only modest VSWR performance (VSWR < 5) [3] or only work at higher frequency band (0.75–1.5 GHz) and have no detailed specification [5]. Wideband antennas, operating in the lower radio frequency (RF) band include discone antennas, biconical antennas, log-periodic antennas and spiral antennas. These antennas are larger, heavier and more expensive than is practical for a dense PD wireless sensor network comprising many tens or even hundreds of radiometer sensor nodes. The design of radiometer antennas must meet some key requirements such as being light in weight, compact in size, low in manufacturing cost and allowing easy integration with a compact RF receiver. A novel simple structure broadband printed antenna meeting these requirements is presented here for PD detection applications. The compact antenna has satisfactory performance over the frequency band 0.35 GHz to 1.38 GHz with small size of around $\lambda_s/4$ (where λ_s is the wavelength of the lowest frequency of the band, i.e., 0.35GHz).

2. Radiated PD

PD comprises short-duration current pulses that occur predominantly in the first and third quadrants of the power system cycle. The frequency spectrum of the pulses has measurable energy extending well into the gigahertz region and a significant fraction of

this energy is radiated from the conductors close to the PD source. Figure 1a shows a typical PD current pulse. The PD current pulse has short duration of the order of nanoseconds with a measureable energy spectrum extending up to several gigahertz. It is often approximated by a Gaussian waveform with half-amplitude width T_l + T_h [4], given by

$$I(t) = I_0 e^{-(t/t_0)^2} \quad (1)$$

where $t_0 = (T_l + T_h)/2\sqrt{\log 2}$. The rise time T_l is usually less than the fall time T_h.

PD activity occurring inside a closed metallic chamber, e.g. the interior of an item of gas insulated switchgear (GIS) or a transformer tank, results in a radiated signal that has been subject to multiple reflections. Electromagnetic signal radiated by PD current pulses have a time waveform and a frequency spectrum that depends on the impulse response of the radiating structure. Figure 1b shows a measured radiated signal. A cost-effective radiometric detection system is designed to measure PD radiated signal. Compact broadband antenna is a key component of such detection system. The designed antenna has successfully been applied to radiometric WSN for PD detection and location, shown in Figure 2, with good performance.

3. Antenna Design

The antenna has been constructed on FR4 substrate with thickness 1.6 mm and dielectric constant 4.9. The dimensions and constructed prototype are shown in Figure 3. It comprises a rectangular patch on one side of the substrate and a ground plane on the other side. The patch is fed by a 50 Ω microstrip transmission line of width 3 mm (W_2).

In most cases, the well matched antenna is simply represented by a 50 Ω resistive load. For broadband antennas, the matching bandwidth can be achieved by overlapping

several adjacent resonances, each which can be represented by an RLC parallel circuit [6], Figure 4. A smooth transition between adjacent resonances ensures good impedance match over a broad frequency range.

The monopole antenna and ground plane form an equivalent dipole antenna [7]. The simple structure antenna is compact (dimensions 200 mm (W) × 240 mm (L)). The overall size of the antenna configuration is around $\lambda_s/4$ instead of $\lambda_s/2$ for the lower edge of the operating frequency. The low frequency limit is determined by the total effective length of the antenna current distribution, which includes the radiation patch and ground plane [8]. The frequency corresponding to the lower resonance of a rectangular planar monopole can be approximately given by

$$f_r = \frac{144}{L + r_1 + r_2}\,\text{GHz} \tag{2}$$

and

$$r_1 = \frac{A_g}{2\pi\sqrt{\varepsilon_{re}}L_1} \tag{3}$$

$$r_2 = \frac{A_p}{2\pi\sqrt{\varepsilon_{re}}(L - L_1 - L_3)} \tag{4}$$

where A_g and A_p are the area of the ground plane and the radiation patch respectively. $\varepsilon_{re} = (1+\varepsilon_r)/2$ is the effective dielectric constant of the composite dielectric. All dimensions are in millimeters. When the desirable frequency band of antenna is available, the antenna size can be compact by optimizing the area and structure of ground and radiation patch.

Slots of dimensions (W_3 × L_4) are cut into the patch shoulders to electromagnetically couple the patch and ground plane. This significantly increases impedance bandwidth. The patch shoulders and bevels result in gradual variation of the distance from the patch to the ground plane. As a consequence, the impedance change from one resonance to

another is small ensuring good impedance match over a broad frequency range. Figure 5 shows the simulated return loss curves for different slot sizes L_4 when other parameters are kept unchanged. The gap L_3 between patch and ground plane introduces a coupling capacitance that further improves impedance matching over the broadband band [7–9]. The simulated return loss curves with different values of L_3 are plotted in Figure 6. The electromagnetic coupling between the lower edge of the patch and the ground plane can be properly controlled by adjusting L_3. The optimized gap distance is chosen as 2 mm. The leaky current between radiating patch and ground plant results in capacitive coupling. Larger gap L_3 leads to weaker coupling therefore worse impedance matching. The ground plane is an integral part of the radiating configuration and its current distribution significantly affects the overall antenna characteristics. The rectangular notch in the ground plane improves both impedance matching and radiation characteristics at high frequency. Figure 7 and 8 show the simulated return loss for various values of W_1 and L_2 when L_3 is fixed at 2 mm. The simulated return loss curves with different values of W_3 are plotted in Figure 9, which shows that W_3 has a modest effect on antenna performance. Detailed investigation and extensive simulations have been undertaken with CST Microwave Studio to optimise the antenna structure and parameters: L_1 = 40 mm, L_2 = 6 mm, L_3 = 2 mm, L_4 = 43 mm, L_5 = 100 mm, W_1 = 64 mm, W_2 = 3 mm, W_3 = 16 mm, W_4 = 50 mm, W_5 = 68 mm, h = 1.6 mm.

4. Results and Discussions

The measurements were made in an anechoic chamber using a vector network analyzer. Figure 10 shows the measured and simulated return loss. The return loss (S11) -10 dB fractional bandwidth is 119% (from 0.35 to 1.38 GHz). The second resonance occurs at 0.77 GHz in the simulation but is not apparent in the measurement. This could be due to

the effect of the SMA port. The normalized *yz*-plane (E-plane) and *xz*-plane (H-plane) radiation patterns have been simulated and measured at 0.45, 0.7 and 1 GHz, Figure 11–13. The *xz*-plane patterns are approximately omnidirectional over the operating frequency range. The *yz*-plane patterns have generally good symmetry. The symmetry becomes less good at the highest measurement frequency as the dimensions of the antenna become comparable to wave length. Overall, the radiation patterns of the antenna are very similar to those of a conventional monopole antenna. The simulated 3D radiation pattern is shown at 0.55GHz as an example in Figure 14.

The calculated variation of maximum gain with frequency is shown in Figure 15. The gain is 1.7 to 5.1 dBi over the design band. The figure indicates that the proposed antenna has good gain flatness with gain variation of less than 3.5 dBi throughout the entire frequency band. The gain decreases at lower frequency band due to compact antenna size. Antenna gain is proportional to the effective radiation aperture. The antenna efficiency of the proposed antenna is equal to the radiation efficiency minus the return loss. The antenna efficiency has a maximum value of 93% and a minimum value of 54% within the frequency range from 0.35–1.38 GHz. The average antenna efficiency is 81%. It is possible that information about the type and severity of insulation defect resides in the time series of received partial discharge pulses. If such information is to be extracted from the received signals then shape of the pulses must be retained. This implies a linear phase (constant group delay) antenna since such an antenna (assuming constant gain across its passband) will not significantly distort the received signal. In this case pulse dispersion must be minimised and group delay will be important. Figure 15 presents the simulated group delay which varies by less than 2 ns from its mean value over most of the operating frequency band. This means that the

broadband antennas have good transient response in the working band. The table below shows the comparison between the proposed antenna and other reported antennas for PD detection.

5. Conclusion

A compact microstrip-fed planar broadband antenna for PD detection applications has been presented. The antenna satisfies a -10 dB return loss requirement from 0.35 to 1.38 GHz. The radiation pattern is close to that of a simple monopole. Predicted variation in group delay is not more than 2 ns. The proposed broadband antenna provides wider impedance bandwidth than the single or multiple narrowband antenna in [1, 4] and the Hilbert antenna (VSWR < 5) in [3] to collect more PD energy for higher radiometric sensitivity. The antenna is compact, light and inexpensive to manufacture making it suitable for use in a dense sensor network.

Acknowledgements

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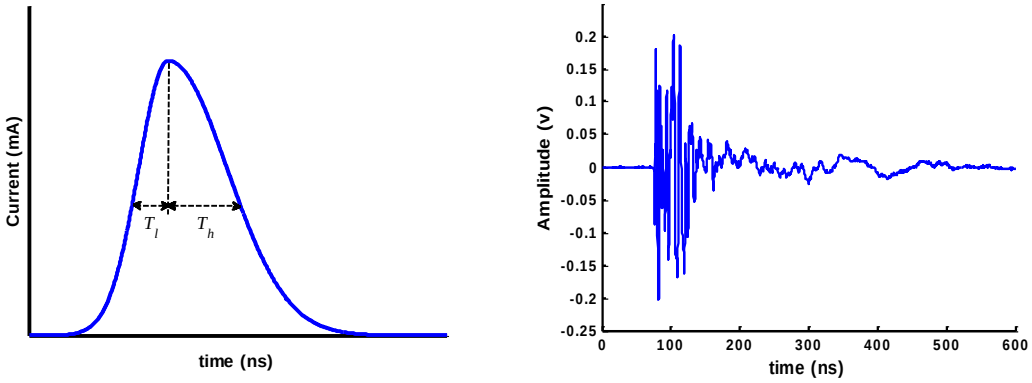

Figure 1. (a) Typical PD current pulse, (b) Typical signal arising from radiated PD energy.

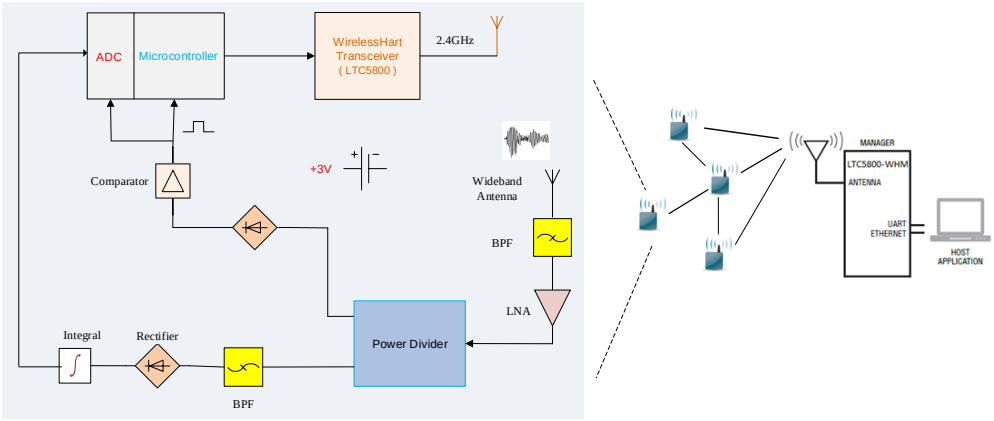

Figure 2. Radiometric wireless sensor network for PD detection and location.

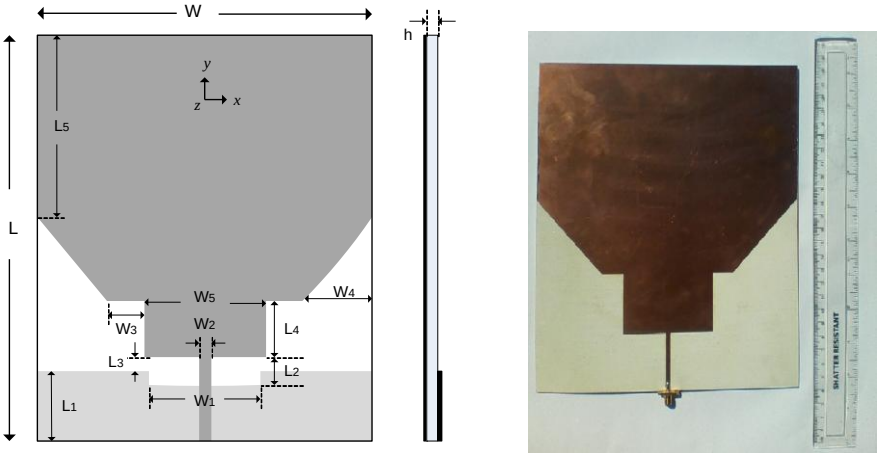

Figure 3. Antenna configuration and constructed prototype

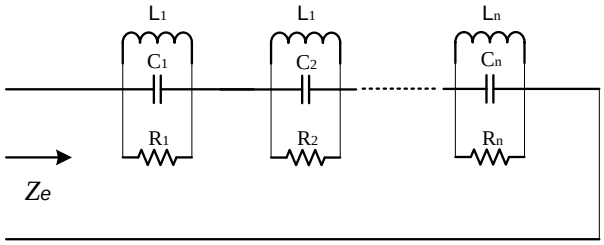

Figure 4. Equivalent circuit model of UWB antenna

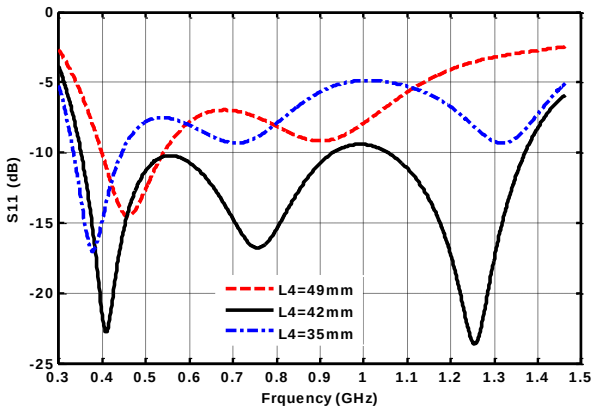

Figure 5. Simulated return loss for different L_4.

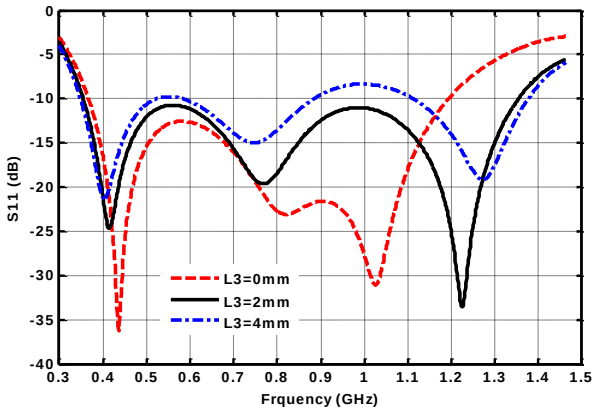

Figure 6. Simulated return loss for different L_3

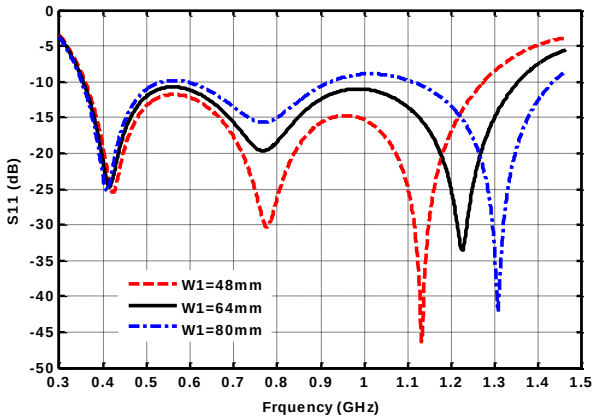

Figure 7. Simulated return loss for different W_1.

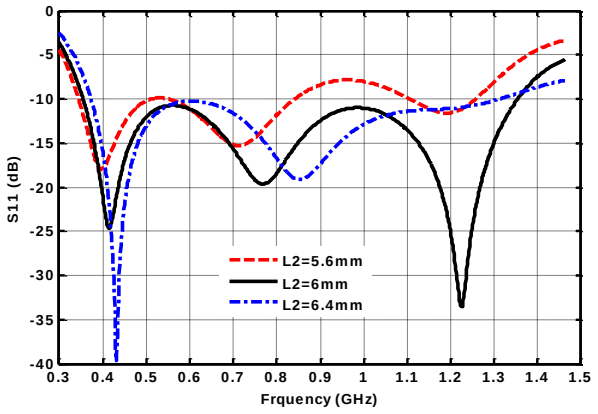

Figure 8. Simulated return loss for different L_2.

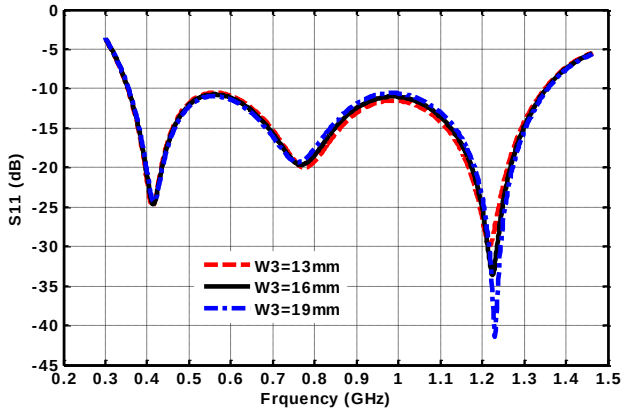

Figure 9. Simulated return loss for different W_3.

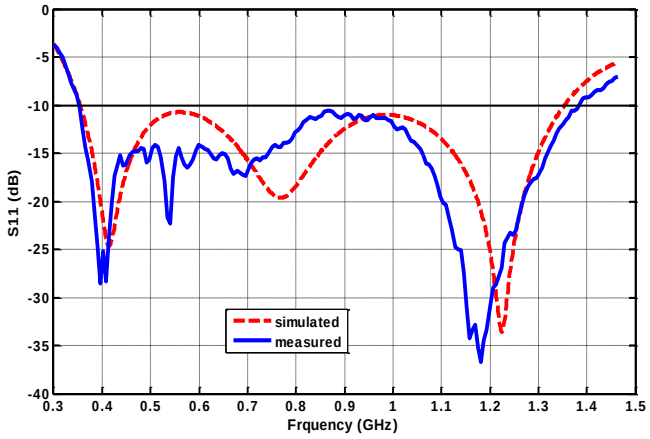

Figure 10. Simulated and measured return loss

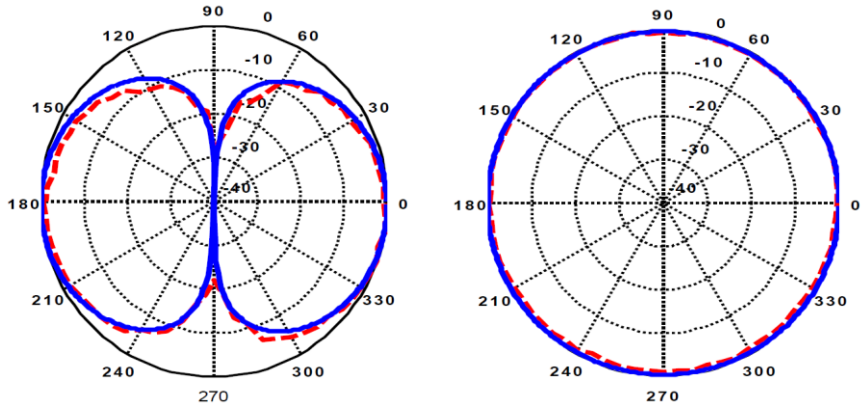

Figure 11. Simulated and measured radiation patterns in the *yz* and *xz* plane at 0.45 GHz. (Solid lines: denote simulations, dashed lines: denote measurements.)

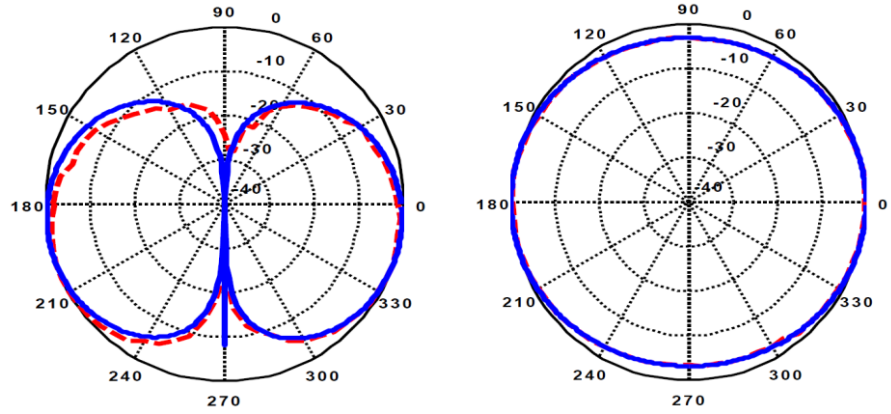

Figure 12. Simulated and measured radiation patterns in the *yz* and *xz* plane at 0.7 GHz. (Solid lines: denote simulations, dashed lines: denote measurements.)

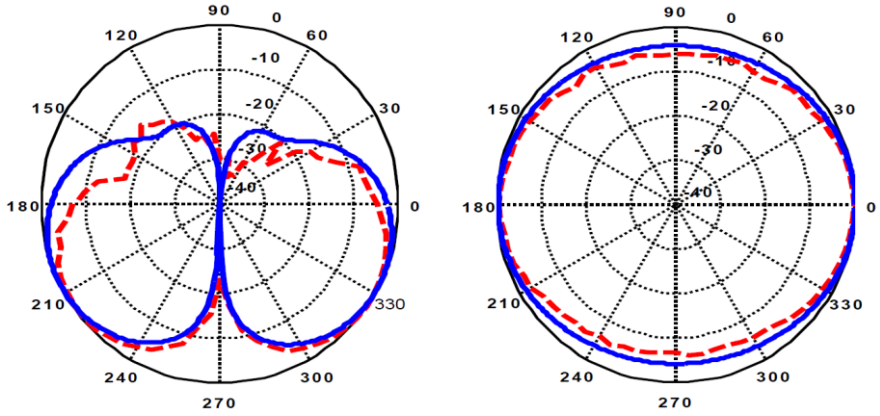

Figure 13. Simulated and measured radiation patterns in the *yz* and *xz* plane at 1 GHz. (Solid lines: denote simulations, dashed lines: denote measurements.)

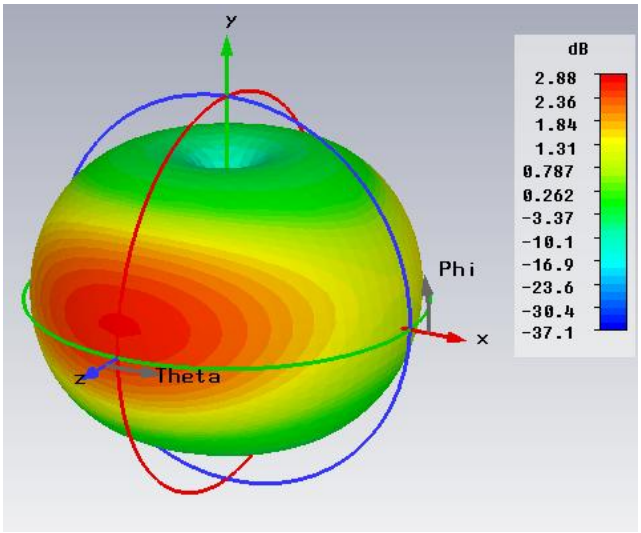

Figure 14. Simulated 3D radiation pattern at 0.55 GHz.

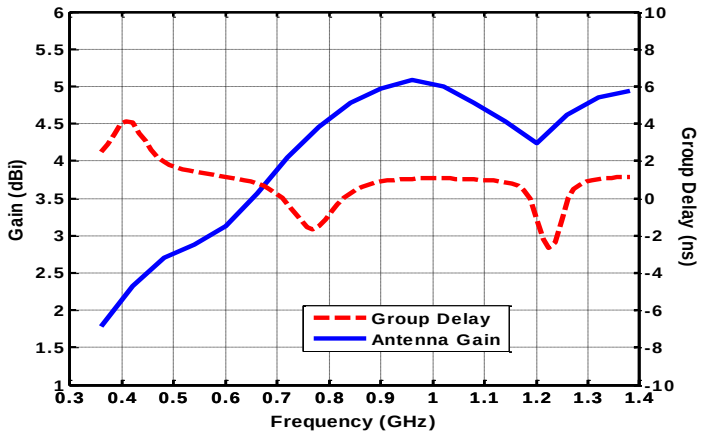

Figure 15. Antenna gain and group delay

Table. Performance comparison of various antennas

Antennas \ parameters	Bandwidth (MHz)	VSWR	Dimension (cm)
The proposed antenna	350 – 1380	< 2	24 × 20
Antenna in Reference 1	480 – 520 800 – 850 1100 – 1200	< 2	19.12 (diameter)
Antenna in Reference 3	339 – 375 395 – 440 450 – 1000	< 5	7 × 7
Antenna in Reference 4	1800 norrowband	< 2	4.19 × 2.94